

# Leaky Capacitors

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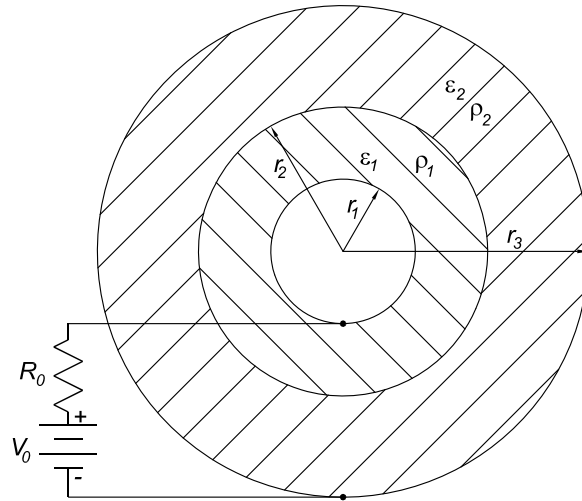
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## 1 Problem

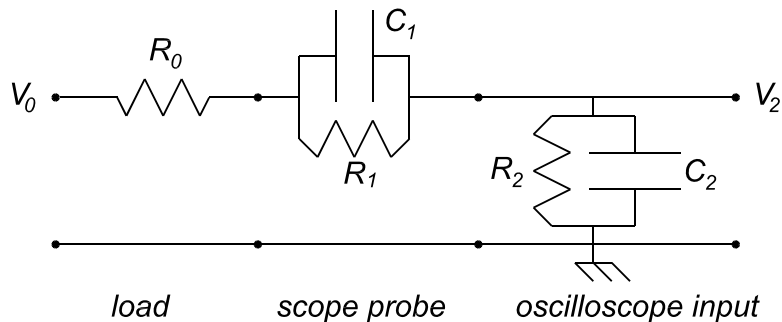
A battery of voltage  $V$  and internal resistance  $R_0$  is connected across a pair of “leaky” spherical capacitors that have inner electrode of radius  $r_1$ , intermediate electrode of radius  $r_2$ , and outer electrode of radius  $r_3$  and whose gaps are filled with concentric shells of dielectrics of differing permittivities,  $\epsilon_1$  for  $r_1 < r < r_2$  and  $\epsilon_2$  for  $r_2 < r < r_3$ . The dielectrics are not perfect insulators but have resistivities  $\rho_1$  and  $\rho_2$ , respectively.



Find the voltage  $V_2(t)$  of electrode 2 supposing that the battery is connected at time  $t = 0$ .

*The human body contains about  $10^{16}$  “leaky capacitors” = the synapses of your nervous system.*

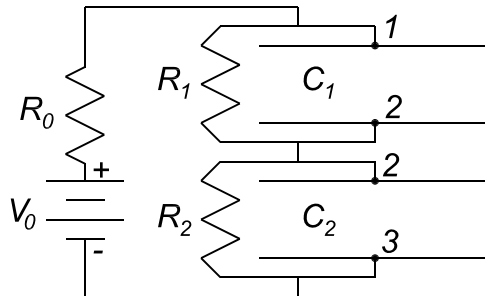
*An application of a pair of “leaky capacitors” is shown below, in which the input circuit of an oscilloscope and a passive probe each include a capacitor and resistor in series.*



## 2 Solution

### 2.1 Resistance and Capacitance

Each of the spherical shells is equivalent to a resistor in parallel with a capacitor, and the two shells are in series, so an equivalent circuit for this problem is as shown below.



The resistance  $R$  of a spherical shell of resistivity  $\rho$ , inner radius  $r_1$  and outer radius  $r_2$  is given by

$$R = \int_{r_1}^{r_2} \frac{\rho dr}{4\pi r^2} = \frac{\rho(r_2 - r_1)}{4\pi r_1 r_2}. \quad (1)$$

To calculate the capacitance  $C$  of a spherical shell capacitor filled with a dielectric of permittivity  $\epsilon$ , consider charge  $Q$  placed on the electrode at radius  $r_1$ , such that the radial electric field is  $E = Q/4\pi r^2$ , and

$$V = \frac{Q}{C} = \int_{r_1}^{r_2} E dr = \int_{r_1}^{r_2} \frac{Q dr}{4\pi \epsilon r^2} = \frac{Q(r_2 - r_1)}{4\pi \epsilon r_1 r_2}, \quad (2)$$

so

$$C = \frac{4\pi \epsilon r_1 r_2}{r_2 - r_1}. \quad (3)$$

In particular,

$$R_1 = \frac{\rho_1(r_2 - r_1)}{4\pi r_1 r_2}, \quad R_2 = \frac{\rho_2(r_3 - r_2)}{4\pi r_2 r_3}, \quad C_1 = \frac{4\pi \epsilon_1 r_1 r_2}{r_2 - r_1}, \quad C_2 = \frac{4\pi \epsilon_2 r_2 r_3}{r_3 - r_2}. \quad (4)$$

### 2.2 One Leaky Capacitor

We first consider the case of a single shell, with resistance  $R$  and capacitance  $C$ .

At large times the current  $I$  is steady, with the value

$$I_\infty = \frac{V}{R_0 + R}, \quad (5)$$

while at  $t = 0$  when the battery is first connected the current is

$$I_0 = \frac{V}{R_0}, \quad (6)$$

since the capacitor appear as a short initially.

Within the shell, the current can be thought of as splitting into two parts that flow through the resistor and capacitor,

$$I(t) = I_R(t) + I_C(t), \quad (7)$$

where  $I_R(0) = 0$ ,  $I_R(\infty) = V_0/(R_0 + R)$ ,  $I_C(0) = V_0/R_0$  and  $I_C(\infty) = 0$ .

The voltage across the shell is given by  $I_R R = Q_C/C$ , whose time derivative is  $\dot{I}_R = I_C/RC$ , so that the total current (7) can be written

$$I = I_R + \dot{I}_R RC. \quad (8)$$

Kirchhoff's law for the entire circuit is now

$$V_0 = I R_0 + I_R R_1 = \dot{I}_R R_0 RC + I_R (R_0 + R), \quad (9)$$

which implies that the current in resistor  $R$  is

$$I_R(t) = \frac{V_0}{R_0 + R} \left(1 - e^{-(R_0+R)t/R_0 RC}\right). \quad (10)$$

Hence, the current in the capacitor is

$$I_C(t) = RC \dot{I}_R = \frac{V_0}{R_0} e^{-(R_0+R)t/R_0 RC}, \quad (11)$$

and the total current is

$$I(t) = \frac{V_0}{R_0 + R} \left(1 - e^{-(R_0+R)t/R_0 RC}\right) + \frac{V_0}{R_0} e^{-(R_0+R)t/R_0 RC} = \frac{V_0}{R_0 + R} \left(1 + \frac{R}{R_0} e^{-(R_0+R)t/R_0 RC}\right). \quad (12)$$

### 2.3 Two Leaky Capacitors

In the case of the original problem with two shells, each with resistance  $R_i$  and capacitance  $C_i$ ,  $i = 1, 2$ , the steady current at long times is

$$I(\infty) = \frac{V_0}{R_0 + R_1 + R_2}. \quad (13)$$

The splitting of the current within each shell can now be written

$$I = I_{R_1} + I_{C_1} = I_{R_2} + I_{C_2}. \quad (14)$$

Extrapolating the form (10) to the case of two shells, we anticipate the presence of two time constants  $\tau_i$ ,

$$I_{R_i} = \frac{V_0}{R_0 + R_1 + R_2} \left(1 - \alpha_i e^{-t/\tau_\alpha} - \beta_i e^{-t/\tau_\beta}\right), \quad (15)$$

where

$$\alpha_i + \beta_i = 1, \quad (16)$$

so that  $I_{R_i}(\infty) = I(\infty) = V_0/(R_0 + R_1 + R_2)$ . Both exponentials  $e^{-t/\tau_\alpha}$  and  $e^{-t/\tau_\beta}$  appear in both currents  $I_{R_i}$  so that eq. (14) can hold at all times.

The currents in the capacitors are

$$I_{C_i} = R_i C_i \dot{I}_{R_i} = \frac{V_0 R_i C_i}{R_0 + R_1 + R_2} \left( \frac{\alpha_i}{\tau_\alpha} e^{-t/\tau_\alpha} + \frac{\beta_i}{\tau_\beta} e^{-t/\tau_\beta} \right). \quad (17)$$

The initial condition on the currents in the capacitors are that  $I_{C_i}(0) = V_0/R_0$ , so we obtain two constraints,

$$\frac{\alpha_i}{\tau_\alpha} + \frac{\beta_i}{\tau_\beta} = \frac{R_0 + R_1 + R_2}{R_0 R_i C_i} \equiv \frac{1}{T_i}, \quad (18)$$

where

$$T_i = \frac{R_0}{R_0 + R_1 + R_2} \tau_i, \quad \text{and} \quad \tau_i = R_i C_i. \quad (19)$$

We can express the  $\alpha_i$  and  $\beta_i$  in terms of  $\tau_\alpha$  and  $\tau_\beta$  using eq. (16) in (18),

$$\alpha_i = \frac{\tau_\alpha}{\tau_\beta - \tau_\alpha} \frac{\tau_\beta - T_i}{T_i}, \quad \text{and} \quad \beta_i = \frac{\tau_\beta}{\tau_\alpha - \tau_\beta} \frac{\tau_\alpha - T_i}{T_i}. \quad (20)$$

Two more constraints are needed to deduce  $\tau_\alpha$  and  $\tau_\beta$ . One of these can be obtained by using eqs. (15) and (17) in (14),

$$\alpha_1 \left( \frac{\tau_1}{\tau_\alpha} - 1 \right) e^{-t/\tau_\alpha} + \beta_1 \left( \frac{\tau_1}{\tau_\beta} - 1 \right) e^{-t/\tau_\beta} = \alpha_2 \left( \frac{\tau_2}{\tau_\alpha} - 1 \right) e^{-t/\tau_\alpha} + \beta_2 \left( \frac{\tau_2}{\tau_\beta} - 1 \right) e^{-t/\tau_\beta}. \quad (21)$$

For this to hold at all times, we must have

$$\alpha_1 (\tau_1 - \tau_\alpha) = \alpha_2 (\tau_2 - \tau_\alpha) \quad \text{and} \quad \beta_1 (\tau_1 - \tau_\beta) = \beta_2 (\tau_2 - \tau_\beta). \quad (22)$$

Using this in eq. (20) we find

$$T_2 (\tau_1 - \tau_\alpha) (\tau_\beta - T_1) = T_1 (\tau_2 - \tau_\alpha) (\tau_\beta - T_2), \quad (23)$$

and

$$T_2 (\tau_1 - \tau_\beta) (\tau_\alpha - T_1) = T_1 (\tau_2 - \tau_\beta) (\tau_\alpha - T_2). \quad (24)$$

From either eq. (23) or (24) we have

$$\tau_\beta = \frac{T_1 T_2 (\tau_1 - \tau_2)}{\tau_1 T_2 - \tau_2 T_1 + \tau_\alpha (T_1 - T_2)} = \frac{T_1 T_2 (\tau_1 - \tau_2)}{\tau_\alpha (T_1 - T_2)} = \frac{R_0 \tau_1 \tau_2}{\tau_\alpha (R_0 + R_1 + R_2)}, \quad (25)$$

recalling eq. (19).

The final constraint can be obtained from Kirchhoff's law for the loop containing resistors  $R_0$ ,  $R_1$  and  $R_2$ ,

$$\begin{aligned} V_0 &= I R_0 + I_{R_1} R_1 + I_{R_2} R_2 \\ &= I_{R_1} (R_0 + R_1) + I_{C_1} R_0 + I_{R_2} R_2 \\ &= V_0 + \frac{V_0 e^{-t/\tau_\alpha}}{(R_0 + R_1 + R_2) \tau_\alpha} [\alpha_1 (R_0 R_1 C_1 - (R_0 + R_1) \tau_\alpha) - \alpha_2 R_2 \tau_\alpha] \\ &\quad + \frac{V_0 e^{-t/\tau_\beta}}{(R_0 + R_1 + R_2) \tau_\beta} [\beta_1 (R_0 R_1 C_1 - (R_0 + R_1) \tau_\beta) - \beta_2 R_2 \tau_\beta]. \end{aligned} \quad (26)$$

For this to be true at all times, each of the quantities in brackets must vanish. Using, for example, the second bracket together with eqs. (20) and (25) we find (after dividing out the common factor  $R_0R_1C_1$ ) a quadratic equation for  $\tau_\alpha$ ,

$$\tau_\alpha^2 - A\tau_\alpha + B = 0, \quad (27)$$

where

$$A = \frac{(R_0 + R_2)R_1C_1 + (R_0 + R_1)R_2C_2}{R_0 + R_1 + R_2} = \frac{R_0(\tau_1 + \tau_2) + R_1\tau_2 + R_2\tau_1}{R_0 + R_1 + R_2}, \quad (28)$$

and

$$B = \frac{R_0R_1C_1R_2C_2}{R_0 + R_1 + R_2} = \frac{R_0\tau_1\tau_2}{R_0 + R_1 + R_2}. \quad (29)$$

The quadratic equation (27) has two positive roots,

$$\tau_\alpha = \frac{A + \sqrt{A^2 - 4B}}{2}, \quad \text{and} \quad \tau_\beta = \frac{A - \sqrt{A^2 - 4B}}{2} = \frac{B}{\tau_\alpha}, \quad (30)$$

recalling eq. (25). As a check, note that if  $R_2 = C_2 = 0$  then  $B = 0$  and  $\tau_\alpha = A = R_0R_1C_1/(R_0 + R_1)$ , as found in eq. (11).

We note that  $\tau_\alpha\tau_\beta = B$ , so that eq. (19) can be rewritten as  $T_i = B/\tau_{3-i}$ , and eq. (20) becomes

$$\alpha_i = \frac{\tau_\alpha - \tau_{3-i}}{\tau_\alpha - \tau_\beta}, \quad \text{and} \quad \beta_i = -\frac{\tau_\beta - \tau_{3-i}}{\tau_\alpha - \tau_\beta}. \quad (31)$$

Finally, the voltage of electrode 2 follows from eq. (15) as

$$V_2 = I_{R_2}R_2 = \frac{V_0R_2}{R_0 + R_1 + R_2} \left( 1 - \frac{\tau_\alpha - \tau_1}{\tau_\alpha - \tau_\beta} e^{-t/\tau_\alpha} + \frac{\tau_\beta - \tau_1}{\tau_\alpha - \tau_\beta} e^{-t/\tau_\beta} \right). \quad (32)$$

A special case is that  $R_1 = R_2 = R/2$  and  $C_1 = C_2 = 2C$ , which reduces to the example (sec. 2.1) of a single shell of resistance  $R$  and capacitance  $C$ . There are still two time constants from eqs. (25) and (30),  $\tau_\alpha = RC$  and  $\tau_\beta = R_0RC/(R_0 + R)$ , of which  $\tau_\beta$  is the one that appears in eq. (11). Then, according to eq. (20),  $\alpha_i = 0$  and  $\beta_i = 1$ , so the time constant  $\tau_\alpha$  does not appear in the current.

Another special case is that  $\tau_1 = R_1C_1 = R_2C_2 = \tau_2 \equiv \tau$ . Then, eq. (20) tells us that  $\alpha_1 = \alpha_2$  and  $\beta_1 = \beta_2$ , and eq. (26) indicates that  $\tau_\alpha = \tau_\beta = \tau R_0/(R_0 + R_1 + R_2)$ . The current  $I$  has the form (12) where  $R = R_1 + R_2$ .

## 2.4 Oscilloscope and Probe

As shown in the lower figure on p. 1, an oscilloscope with a capacitive probe is an application of a pair of “leaky capacitors”.

Here, we are particularly concerned with the response voltage,  $V_2(\omega)$ , at the oscilloscope input to a sinusoidal load voltage  $V_0e^{i\omega t}$ . Noting that the impedance  $Z_{\parallel}$  of a resistor  $R$  in parallel with a capacitor  $C$  is

$$Z_{\parallel} = \frac{R}{1 + i\omega\tau}, \quad (33)$$

where  $\tau = RC$ , we have

$$V_2(\omega) = IZ_2 = V_0 \frac{Z_2}{Z} = V_0 \frac{Z_2}{R_0 + Z_1 + Z_2} = V_0 \frac{R_2}{R_0(1 + i\omega\tau_2) + R_1 \frac{1+i\omega\tau_2}{1+i\omega\tau_1} + R_2}. \quad (34)$$

In practice, the resistances  $R_1$  and  $R_2$  should be large compared to  $R_0$ , in which case the probe acts as a frequency-independent voltage divider,

$$V_2 \approx V_0 \frac{R_2}{R_1 + R_2}, \quad (35)$$

provided  $R_1C_1 = \tau_1 = \tau_2 = R_2C_2$ .

## 2.5 Solution via Laplace Transforms

The frequency response (34) can be used to deduce the transient response to a constant voltage  $V_0$  that is turned on at  $t = 0$  via the techniques of Laplace transforms.

### 2.5.1 Definition of the Laplace Transform

Recall that in general a function  $f(t)$  can be represented as a Fourier integral,

$$f(t) = \int_{-\infty}^{\infty} f_{\omega} e^{i\omega t} d\omega, \quad (36)$$

where the Fourier amplitude  $f_{\omega}$  is given by

$$f_{\omega} = \frac{1}{2\pi} \int_{-\infty}^{\infty} f(t) e^{-i\omega t} dt. \quad (37)$$

For the special case that  $f(t) = 0$  for  $t < 0$ , the Fourier amplitude is

$$f_{\omega} = \frac{1}{2\pi} \int_0^{\infty} f(t) e^{-i\omega t} dt. \quad (38)$$

We can define  $s = i\omega$ , and introduce the Laplace transform  $F(s)$  of the function  $f(t)$  as

$$F(s) = 2\pi f_{\omega} = \int_0^{\infty} f(t) e^{-st} dt, \quad (39)$$

in which case the Fourier integral (36) can be rewritten as<sup>1</sup>

$$f(t) = \frac{1}{2\pi} \int_{-\infty}^{\infty} F(s) e^{i\omega t} d\omega = \frac{1}{2\pi i} \int_{-i\infty}^{i\infty} F(s) e^{st} ds, \quad (40)$$

which relation is called the inverse Laplace transform.

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<sup>1</sup>Strictly, the integration is along a contour in the complex  $s$  plane that includes a line along some value of  $Re(s)$  such that all poles of  $F(s)$  lie within the contour when it is closed to the left via an infinite half circle.

## 2.5.2 Analysis of Impulse Response

We now use the method of Laplace transforms for the example of oscilloscope and probe to determine the response waveform  $V_2(t)$  from the driving waveform  $V_0(t)$ . A first approach follows the spirit of Green by supposing  $V_0(t)$  is the Dirac delta function  $\delta(t)$ , *i.e.*, a brief impulse of voltage.

From eq. (38) we see that all Fourier components of  $\delta(t)$  are the same, namely  $1/2\pi$  since  $\int \delta(t)f(t) dt = f(0)$ . From eq. (39) the Laplace transform of the delta function is 1. Hence, dividing eq. (34) by  $2\pi V_0$  gives the Fourier component of the response voltage  $V_{2,\text{impulse}}$  caused by the impulse  $\delta(t)$ . Then, eq. (39) tells us that  $V_2(\omega)$  is the Laplace transform of the response function, so we rewrite eq. (34) using  $s = i\omega$  as

$$\begin{aligned} F_{2,\text{impulse}}(s) &= V_2(\omega) = V_0 \frac{R_2(1 + s\tau_1)}{R_0(1 + s\tau_1)(1 + s\tau_2) + R_1(1 + s\tau_2) + R_2(1 + s\tau_1)} \\ &= \frac{V_0 R_2}{R_0 \tau_2} \frac{s + 1/\tau_1}{(s - \sigma_\alpha)(s - \sigma_\beta)}, \end{aligned} \quad (41)$$

where  $\sigma_\alpha$  and  $\sigma_\beta$  are the roots of the quadratic equation

$$s^2 + \frac{R_0(\tau_1 + \tau_2) + R_1\tau_1 + R_2\tau_1}{R_0\tau_1\tau_2}s + \frac{R_0 + R_1 + R_2}{R_0\tau_1\tau_2} = s^2 + \frac{A}{B}s + \frac{1}{B} = 0, \quad (42)$$

where the constants  $A$  and  $B$  were introduced in eqs. (28)-(29). That is,

$$\sigma_\alpha = -\frac{A - \sqrt{A^2 - 4B}}{2B} = -\frac{1}{\tau_\alpha}, \quad \text{and} \quad \sigma_\beta = -\frac{A + \sqrt{A^2 - 4B}}{2B} = -\frac{1}{\tau_\beta}, \quad (43)$$

recalling eq. (30).

To find  $V_{3,\text{impulse}}(t)$ , we note that the inverse Laplace transform of the form

$$F(s) = \frac{s + c}{(s + a)(s + b)} \quad (44)$$

is

$$f(t) = \frac{(c - a)e^{-at} - (c - b)e^{-bt}}{b - a}. \quad (45)$$

Using this with eqs. (41) and (43), we obtain the form of the impulse response

$$\begin{aligned} V_{2,\text{impulse}}(t) &= \frac{R_2}{R_0\tau_2} \frac{(1/\tau_1 - 1/\tau_\alpha)e^{-t/\tau_\alpha} - (1/\tau_1 - 1/\tau_\beta)e^{-t/\tau_\beta}}{1/\tau_\beta - 1/\tau_\alpha} \\ &= \frac{R_2}{R_0\tau_1\tau_2} \frac{\tau_\beta(\tau_\alpha - \tau_1)e^{-t/\tau_\alpha} - \tau_\alpha(\tau_\beta - \tau_1)e^{-t/\tau_\beta}}{\tau_\alpha - \tau_\beta}. \end{aligned} \quad (46)$$

The response  $V_2(t)$  to any drive voltage  $V_0(t)$  can be deduced from the impulse response,

$$V_2(t) = \int_{-\infty}^t V_0(t')V_{2,\text{impulse}}(t - t') dt'. \quad (47)$$

In particular, the response  $V_{2,\text{step}}(t)$  to a step in voltage from 0 at  $t, 0$  to  $V_0$  for  $t > 0$  is

$$\begin{aligned}
V_{2,\text{step}}(t) &= V_0 \int_0^t V_{2,\text{impulse}}(t-t') dt' = V_0 \int_0^t V_{2,\text{impulse}}(t'') dt'' \\
&= \frac{V_0 R_2}{R_0 \tau_1 \tau_2} \left[ \frac{\tau_\beta (\tau_\alpha - \tau_1)}{\tau_\alpha - \tau_\beta} \int_0^t e^{-t''/\tau_\alpha} dt'' - \frac{\tau_\alpha (\tau_\beta - \tau_1)}{\tau_\alpha - \tau_\beta} \int_0^t e^{-t''/\tau_\beta} dt'' \right] \\
&= \frac{V_0 R_2 \tau_\alpha \tau_\beta}{R_0 \tau_1 \tau_2 (\tau_\alpha - \tau_\beta)} \left[ (\tau_\alpha - \tau_1)(1 - e^{-t/\tau_\alpha}) - (\tau_\beta - \tau_1)(1 - e^{-t/\tau_\beta}) \right] \\
&= \frac{V_0 R_2}{R_0 + R_1 + R_2} \left( 1 - \frac{\tau_\alpha - \tau_1}{\tau_\alpha - \tau_\beta} e^{-t/\tau_\alpha} + \frac{\tau_\beta - \tau_1}{\tau_\alpha - \tau_\beta} e^{-t/\tau_\beta} \right), \tag{48}
\end{aligned}$$

as found previously in eq. (32).

Equation (47) can be re-expressed in the language of Laplace transforms on noting that there is no response prior to the drive impulse, so  $V_{2,\text{impulse}}(t) = 0$  for  $t < 0$ . Hence, we can extend the limit of integration in eq. (47) from  $t$  to  $\infty$ ,

$$V_2(t) = \int_{-\infty}^{\infty} V_0(t') V_{2,\text{impulse}}(t-t') dt'. \tag{49}$$

The Laplace transform  $F_2(s)$  of eq. (49) is (assuming that  $V_0(t) = 0$  for  $t < 0$ )

$$\begin{aligned}
F_2(s) &= \int_0^{\infty} e^{-st} dt \int_{-\infty}^{\infty} V_0(t') V_{2,\text{impulse}}(t-t') dt' \\
&= \int_{-\infty}^{\infty} V_0(t') e^{-st'} dt' \int_{-\infty}^{\infty} V_{2,\text{impulse}}(t-t') e^{-s(t-t')} dt \\
&= \int_0^{\infty} V_0(t') e^{-st'} dt' \int_0^{\infty} V_{2,\text{impulse}}(t'') e^{-st''} dt'' \\
&= F_0(s) \cdot F_{2,\text{impulse}}(s). \tag{50}
\end{aligned}$$

Thus, the Laplace transform  $F_{2,\text{impulse}}(s)$  of the response  $V_{2,\text{impulse}}(t)$  to a drive impulse at  $t = 0$  equals the Laplace transform  $F_2(s)$  of the response  $V_2(t)$  to any drive waveform  $V_0(t)$  (provided  $V_0(t) = 0$  for  $t < 0$ ) divided by the Laplace transform  $F_0(s)$  of that drive waveform,

$$\frac{F_2(s)}{F_0(s)} = F_{2,\text{impulse}}(s) \equiv \text{transfer function}. \tag{51}$$

The ratio of the Laplace transform of the response function to the Laplace transform of the drive function is called the transfer function. Thus, eq. (41) describes the transfer function for the present example.

### 2.5.3 Step Response via the Impulse Response Transform

The response to a step driving term can also be found by a slightly different procedure. We note that the delta function  $\delta(t)$  is the time derivative of the Heaviside step function,

$$\delta(t) = \frac{d\theta}{dt}, \quad \text{where} \quad \theta(t) = \begin{cases} 0 & (t < 0), \\ 1 & (t > 0). \end{cases} \tag{52}$$

We also see from eq. (39) that the Laplace transform of the time derivative  $df/dt$  is  $s$  times the Laplace transform of function  $f(t)$ ,

$$\int_0^{\infty} \frac{df}{dt} e^{-st} dt = f e^{-st} \Big|_0^{\infty} + s \int_0^{\infty} f e^{-st} dt = sF(s). \quad (53)$$

Hence, the Laplace transform of the step response is equal to the Laplace transform of the impulse response divided by  $s$ . *Recalling the discussion at the end of sec. 2.5.2, this relation can also be stated as: the Laplace transform of the step response is equal to the transfer function divided by  $s$ .*

On dividing the transfer function (41) by  $s$ , the Laplace transform of the response  $V_{2,\text{step}}$  to a step in voltage  $V_0$  is

$$\frac{V_0 R_2}{R_0 \tau_2} \frac{s + 1/\tau_1}{s(s + 1/\tau_\alpha)(s + 1/\tau_\beta)}. \quad (54)$$

The inverse of the Laplace transform

$$\frac{s + c}{s(s + a)(s + b)} \quad (55)$$

is<sup>2</sup>

$$f(t) = \frac{c}{ab} \left( 1 - \frac{b(c-a)}{a-b} e^{-at} + \frac{a(c-b)}{a-b} e^{-bt} \right). \quad (56)$$

The particular form (54) then leads immediately to the step response (32) and (48).

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<sup>2</sup>See, for example, D. Christiansen, R. Jurgen and D. Fink, *Electronics Engineers' Handbook*, 4th ed. (McGraw-Hill, New York, 1996).